# Fourier Convolution Operation on Metasurface-Based Hologram in Microwave Region 

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#### Abstract

In this paper, a $0.1 \lambda_{0}$-thick 1-bit coding metasurface is proposed to achieve a polarizationinsensitive hologram under oblique incidence, utilizing compact ground-backed patch unit cells. Fourier convolution theory in a digital signal processing system is added to the hologram calculation of the improved weighted Gerchberg-Saxton (GSW) algorithm to achieve control of the scattered pattern in the microwave region. As a proof of concept, a prototype operating at 15 GHz is designed to verify the validity of our proposed approach. The measured performances show good imaging quality under different incident polarizations, providing potential applications in imaging processing and information storage.


Keywords: metasurface; polarization-insensitive; hologram

## 1. Introduction

Metasurfaces, the two-dimensional (2D) version of metamaterials, are composed of arrays of artificial scatters, known as meta-atoms, with designed geometries and orientation angles, which allow one to control the main characteristics of the scattered wave such as amplitude, phase and polarization [1,2]. Due to the extraordinary capability of tailoring wavefronts and low loss, low cost and low profile characteristics, metasurfaces have been extensively exploited in practical devices, such as retroreflectors [3], cloaking devices [4], orbital angular momentum (OAM) generators [5], flat lenses [6], and holograms [7-10], to name a few. Recently, the concept of coding metasurface has attracted much attention, in which the phase or amplitude response of the metasurface is characterized by N -bit digital coding particles rather than continuous electromagnetic (EM) parameters. For example, using the simplest 1-bit coding of the binary coding scheme, elements of the reflective metasurface are " 0 " and " 1 ", corresponding to phase response 0 and $\pi$, respectively. Electromagnetic waves can be manipulated in a simple and effective way by designing the encoding sequence of digital meta-atoms, which has many applications in beam forming [11], diffuse scattering [12], energy radiations control [13] and complex wavefront shaping [14]. Holography is one of the most promising imaging techniques [15]. Traditional holograms can be generated by the interference of a reference beam and the scattered beam from the real object or calculated by using numerical computation [16,17]. Compared with traditional holograms, the emergence of metasurfaces has further promoted the development of computational holographic imaging by providing unprecedented spatial resolution, and high-precision reconstructed images. By introducing a reconstruction algorithm such as Gerchberg-Saxton (GS) [18], computer-generated holograms can be designed using engineered sub-wavelength elementary atoms with well-tailored amplitude and phase responses, and digital elementary holography can be generated by coding the holographic information of the object pattern [7,8]. Compared with traditional geometric
optics, the spatial resolution and imaging rate of metasurface holographic imaging are significantly improved. Due to the precise control of EM waves, holographic metasurface also finds applications in short-range communication systems, detection, data storage, and information processing [19-21] in the microwave regime.

Efficiency is one of the most important challenges in metasurface design. Due to basic limitations and inherent ohmic losses, the efficiency of a single-layer transmissive metasurface is often fairly low, and has been shown to be only of the order of a few percent of magnitude at most [2]. Some high-efficiency transmissive metasurfaces, for instance, dielectric metasurfaces [22], Huygens' metasurfaces [23], multilayered metasurfaces and meta-transmitarrays [24,25], have been studied to improve the efficiency. However, these designs necessitate a minimum finite thickness, significant manufacturing complexities and frequency dispersions. Reflective metasurfaces provide a solution for high-efficiency and ultrathin metasurface design and have been demonstrated in various applications such as antennas [26-29], holograms [30,31], waveplates [32] and metamirrors [33,34]. However, the feeding source of reflective metasurfaces is usually in the path of the reflected signal, which affects the performances of the metasurfaces.

Recently, we proposed the coding metasurface approach for enhanced quality holographic imaging by discretizing the phase distribution calculated by a GSW algorithm to different bit levels $[7,8]$. In this paper, a reflective 1-bit coding metasurface is proposed for polarization-insensitive hologram under oblique incidence of $60^{\circ}$ in the microwave region, as illustrated in Figure 1a. The proposed metasurface is composed of subwavelength patch elements, which can provide a $180^{\circ}$ phase shift for dual linearly polarized incidences. By designing the size of the patch elements, we find the meta-atoms of the binary element codes " 0 " and " 1 " to construct a 1 -bit coding element hologram. A modified GSW algorithm is used to calculate the original interfacial phase distribution. Then, by applying Fourier convolution operations on the hologram, the direction of the scattered pattern can be steered to the desired direction. Experimental verification performed on a fabricated prototype is qualitatively consistent with theoretical predictions and numerical simulations, demonstrating both the feasibility of the approach and the high imaging quality of the proposed 1-bit polarization-insensitive coding element hologram.
(a)

(c)

(b)
(d) TE incidence at 15 GHz


Figure 1. Cont.


Figure 1. (a) Schematic demonstration of the proposed 1-bit polarization-insensitive metasurfacebased hologram under oblique incidence. (b) 3D topological structure of the unit cell. (c,d) Reflection phase response of the meta-atom under TM and TE polarization as functions of $P_{x}$ and $P_{y}$, respectively. (e,f) Reflection coefficients of the binary meta-atoms as a function of frequency under TM and TE polarization, respectively.

## 2. Design of the Coding Elements

Figure 1a shows the schematic diagram of a hologram of arbitrary polarization at a large incidence angle of $60^{\circ}$. By introducing Fourier convolution operation on the metasurface, the scattering pattern of the hologram can be steered as desired. For the convenience of measurement, the hologram is designed to scatter in the normal direction here. Figure 1b shows the geometry and parameters of the coding particles. The F4BM300 dielectric substrate with thickness $t=2 \mathrm{~mm}$, relative permittivity $\varepsilon_{\mathrm{r}}=3$ and $\tan \delta=0.0015$ is used. A ground-backed patch meta-atom is exploited as the coding particle due to its good performance in polarization isolation and fabrication tolerance requirements. The perfect electric conductor (PEC) boundary condition is considered for the metal parts in simulations. Numerical simulations are performed using the commercial software CST Microwave Studio. Under the incidence of TM wave, the phase response of the meta-atom varies with the length $P_{x}$ of the patch along the $x$-direction, as shown in Figure 2c. It can also be observed that the length $P_{y}$ of the patch along $y$-direction has little influence on the phase response. The reflection phase coverage approaches $210^{\circ}$ for TM incidences by varying the length $P_{x}$. Similarly, a reflection phase coverage of $310^{\circ}$ is obtained by varying the length $P_{y}$. The phase coverages under dual linearly polarized incidences are efficient to achieve a $180^{\circ}$ phase shift for the unit cell design. A bare unit cell (without metal patch element) is utilized here to operate as code " 0 " to simplify the design process and also to reduce the coupling effect between adjacent unit cells. To satisfy the $180^{\circ}$ phase shift between code " 0 " and code " 1 " under dual linearly polarized incidences, the parameters of unit cell code " 1 " is optimized to be $P_{x}=5.2 \mathrm{~mm}$ and $P_{y}=3.4 \mathrm{~mm}$.
(a)


(b)

(c)

(d)


Figure 2. (a) Phase distribution of the original hologram. (b) Gradient phase distribution. (c) Phase distribution of hologram in normal direction. (d) 1-bit coding map.

Figure 1e,f shows the reflection responses of the binary unit cells under TM and TE incidences as a function of frequency. For the dual linear polarizations, a phase difference of $180^{\circ}$ is achieved at 15 GHz , providing the freedom to have the same phase shift in both TE and TM polarizations sharing the same aperture. The reflection amplitudes can also be nearly uniform under the different polarizations, as shown in Figure 1e,f. Since arbitrary polarizations can be decomposed into TE and TM polarizations, the same hologram for any polarization can be obtained from the metasurface.

## 3. Design of the Coding Meta-Hologram

The modified GSW algorithm is used to retrieve the required theoretical phase profile [2]. The method consists in selecting ideal point sources as virtual sources and placing them at pre-designed hotspots. Considering that there are $N$ hotspots located at ( $x_{n}, y_{n}$, $\left.z_{n}\right)(n=1$ to $N)$, the phase delay at the position of each coding element $\phi\left(x_{m}, y_{m}, z_{m}\right)$ ( $m=1$ to $M$ ) can be retrieved by superposing the electromagnetic field generated by all the virtual sources described by Green's function. Accordingly, the reconstructed electric field is converged to the predesigned hotspots. In order to keep uniform intensity distribution among hotspots, a weight factor $w_{n}$ is introduced to reduce intensity difference among the $N$ hotspots. An iterative procedure between the holography imaging and meta-hologram is proposed to obtain the uniform intensity profile of the target image as follows:

$$
\begin{gather*}
\phi_{m}^{p}=\arg \left(\sum_{n=1}^{N} \frac{e^{i k r_{m}^{n}}}{r_{m}^{n}} \frac{w_{n}^{p} E_{n}^{p-1}}{\left|E_{n}^{p-1}\right|}\right)  \tag{1}\\
E_{n}^{p}=\sum_{m=1}^{M} \frac{e^{-i k r_{m}^{n}+i \phi_{m}^{p}}}{r_{m}^{n}}  \tag{2}\\
w_{n}^{p}=w_{n}^{p-1} \frac{\sum_{n=1}^{N}\left|E_{n}^{p-1}\right|}{N\left|E_{n}^{p-1}\right|} \tag{3}
\end{gather*}
$$

where $\phi_{m}$ is defined as the phase shift of the $m^{\text {th }}(m=1$ to $M)$ coding element and $E_{n}$ denotes the electric field intensity of the $n^{\text {th }}(n=1$ to $N)$ hotspots. $r_{m}^{n}$ is the distance between $m^{\text {th }}$ coding element and $n^{\text {th }}$ hotspot and superscript $p$ represents the $p^{\text {th }}$ iterative step. According to Equations (1) and (3), the weight factor $w_{n}$ is adjusted step by step until the least mean square error between the target and the reconstructed image becomes less than a predesigned threshold. Based on the modified GSW retrieval algorithm, the theoretical phase distribution can be obtained, as shown in Figure 2a.

As a property of the Fourier transform, the convolution theorem can be described:

$$
\begin{equation*}
f(t) \bullet g(t) \stackrel{F F T}{\Leftrightarrow} f(\omega) * g(\omega) \tag{4}
\end{equation*}
$$

The arguments $t$ and $\omega$ in Equation (1) can be replaced by $x_{\lambda}$ and $\sin \theta$, respectively, leading to the following equation [35]:

$$
\begin{equation*}
f\left(x_{\lambda}\right) \bullet g\left(x_{\lambda}\right) \stackrel{F F T}{\Leftrightarrow} f(\sin \theta) * g(\sin \theta) \tag{5}
\end{equation*}
$$

where $x_{\lambda}=x / \lambda$ is the electrical length, and $\theta$ is the angle with respect to the normal direction. Equation (2) can be simplified when the item $\mathrm{g}\left(x_{\lambda}\right)$ becomes a Dirac-delta function:

$$
\begin{gather*}
E\left(x_{\lambda}\right) \bullet e^{j x_{\lambda} \sin \theta_{0}} \stackrel{F F T}{\Leftrightarrow} E(\sin \theta) * \delta\left(\sin \theta-\sin \theta_{0}\right)  \tag{6}\\
=E\left(\sin \theta-\sin \theta_{0}\right)
\end{gather*}
$$

where $x_{\lambda} \sin \theta_{0}$ describes the gradient phase along a determined direction. Equation (3) shows that by introducing a gradient phase of $e^{j x_{\lambda} \sin \theta_{0}}$, the scattering pattern $E\left(\sin \theta_{0}\right)$ can
be deviated from its original direction by the quantity $\sin \theta_{0}$ in the angular coordinate. Such a process can be regarded as superposing an additional phase distribution to the original one, reducing computational complexity for optimizing the scattering patterns. Based on the scattering pattern shift principle, the hologram can be arbitrarily rotated around the normal axis by the convolution operation. Since the incidence angle is designed to be $60^{\circ}$ here, a gradient phase distribution shown in Figure $2 b$ is added to the original hologram to steer the scattering pattern to the normal direction. Then, the obtained phase distribution in Figure 2c is discretized to 0 and $\pi$ values. Therefore, the phase information can be described by the 1-bit coding map shown in Figure 2d. Then, the 1-bit coding hologram can be constructed based on the obtained coding map.

## 4. Results and Discussion

To demonstrate the proposed 1-bit polarization-insensitive hologram, a metasurface is designed at 15 GHz and simulated to project a "square" image with four corner hotspots, as illustrated in Figure 1a. The metasurface is composed of $41 \times 41$ meta-atoms with the size of $235.75 \mathrm{~mm} \times 235.75 \mathrm{~mm}$. The metasurface is fabricated using the conventional printed circuit board (PCB) technique where copper is used for the metal parts. The imaging plane here is designed to be $4 \lambda$ away from the metasurface. The metasurface is illuminated by TM, TE, left-hand circularly polarized (LHCP) and right-hand circularly polarized (RHCP) waves under an oblique incidence angle of $60^{\circ}$. Figure 3a,b, respectively, present the intensity distribution of the simulated reflected electric field in the imaging plane under TM and TE incident waves illumination. Under LHCP and RHCP wave incidences, the simulated reflected electric field strength of the cross-polarized component is shown in Figure $3 c, e$. The simulation results are consistent with the theoretical design, showing good imaging quality. It should be noted that a small part of incident $C P$ wave is transformed into its co-polarized component in the reflected field, as shown in Figure 3d,f, since the reflection phases for TM and TE incidences are not identical, as previously presented in Figure 1e,f.


Figure 3. Simulated reflected electric field intensity distributions ( $\mathbf{a}, \mathbf{b}$ ) under TM and TE incidence, respectively. (c,d) Cross- and co-polarized component under LHCP incidence, respectively. (e,f) Cross- and co-polarized component under RHCP incidence, respectively.

In order to experimentally verify the performances of the proposed polarizationinsensitive hologram, a sample is fabricated and depicted by the photograph shown in the inset of Figure 4a. The schematic diagram of the near-field scanning system exploited to measure the electric field distribution is illustrated in Figure 4a, and the measurements are carried out in a microwave anechoic chamber. The feeding source, which is a dualpolarized broadband horn antenna, is placed far away enough from the metasurface to launch quasi-plane waves (TM, TE, LHCP and RHCP as required) at an oblique incidence angle of $60^{\circ}$. The feeding horn antenna is connected to one port of a vector network analyzer (VNA) and fixed at the angle of $60^{\circ}$. A field-sensing probe is used to measure both the amplitude and the phase of the electric field. From the measured data of the electric field along the $x$ - and $y$-axes, the LHCP and RHCP components are calculated as:

$$
\begin{align*}
& E_{L H C P}=\frac{1}{\sqrt{2}}\left(E_{x}-i E_{y}\right)  \tag{7}\\
& E_{R H C P}=\frac{1}{\sqrt{2}}\left(E_{x}+i E_{y}\right)
\end{align*}
$$

where $E_{x}$ and $E_{y}$ is the electric field along $x$ - and $y$-axis, respectively. $E_{L H C P}$ and $E_{R H C P}$ is the electric field of the LHCP and RHCP component, respectively.


Figure 4. (a) Schematic diagram of the experimental setup used to measure the electric field distribution. A photograph of the fabricated sample is shown in the inset. (b,c) Measured reflected field intensity distribution under TM and TE incidence, respectively. (d,e) Measured reflected electric intensity distribution of the cross- and co-polarized component under LHCP incidence, respectively. $(\mathbf{f}, \mathbf{g})$ Measured reflected electric intensity distribution of the cross- and co-polarized component under RHCP incidence, respectively.

Figure 4 b-g depicts the measured results, showing good qualitative agreement with the simulated ones presented in Figure 3a-f. The imaging efficiency, which refers to the proportion of the total incident energy concentrated in the preset focus, is calculated as the energy in the preset focus referenced to the total reflected energy on the measured plane [7,8]. The imaging efficiency is calculated to be $37.3 \%$ and $40.3 \%$ for TM and TE incidence, respectively. It should be noted that a higher bit level of coding elements can reduce the phase discretization and improve the performance of the metasurface, as it has been demonstrated in a previous work [7]. However, here, the 1-bit coding level is used as a good tradeoff between design complexity and imaging performance. As discussed above, since the reflection phases for TM and TE incidences are not identical, some of the incident CP wave is transformed into its co-polarized component in the reflected field, as shown in Figure 4e,g. The ratio of the co-polarized component on the measured plane to the total reflected energy is measured to be $39.6 \%$ and $35.4 \%$ for LHCP and RHCP
incidence, respectively. The imaging efficiency of the cross- and co-polarized component is measured to be $18.4 \%$ and $11.7 \%$ for LHCP incidence, and $19.9 \%$ and $7.5 \%$ for RHCP incidence. The signal-to-noise ratio (SNR) is used to describe the ratio between the peak intensity in the image and the standard deviation of the background noise $[7,8]$, which is calculated to be $15.7,14.1,13.9,12.9,13.4$ and 11.6 for the measured results shown in Figure $4 b-\mathrm{g}$, respectively.

To further validate the performances of the metasurface when deviating from the preset conditions, the results obtained at different focal distances and incidence angles are shown and discussed. Under oblique incidence different from $60^{\circ}$, the simulated results under y-polarized incidence for $50^{\circ}$ and $70^{\circ}$ incidence are shown in Figure 5, where it can be clearly observed that the proposed metasurface can still achieve reasonable performance. The simulation results at different focal distances of $60 \mathrm{~mm}, 70 \mathrm{~mm}, 90 \mathrm{~mm}$ and 100 mm are also presented in Figure 6. When the focal distance deviates from the designated value, the image quality decreases, owing to the change of phase delay on the focal plane.


Figure 5. Simulated reflected electric intensity distributions under $y$-polarized incidence at different oblique incidence angles: (a) $50^{\circ}$. (b) $70^{\circ}$.


Figure 6. Simulated reflected electric intensity distributions under $y$-polarized incidence at different distances: (a) 60 mm . (b) 70 mm . (c) 90 mm . (d) 100 mm .

## 5. Conclusions

In conclusion, a polarization-insensitive 1-bit metasurface is designed and validated for imaging hologram under oblique incidence in the microwave region. It is also demonstrated that the scattering direction of the hologram can be steered as desired by simply adding a gradient phase distribution based on the Fourier convolution theory. For the arbitrarily considered linear and circular polarized waves, the experimental measurements performed on a fabricated prototype highlight good imaging quality. The proposed ultra-thin polarization-insensitive 1-bit metasurface-based hologram may pave the way to potential applications in imaging processing and information storage.

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